

The Effects of ASE Noise and the Position of EDFA Amplifier on Multi-Wavelength OCDM-Based Long-Reach Passive Optical Networks

Bùi Trung Ninh¹, Phạm Văn Hội², Đặng Thế Ngọc³,
Phạm Tuấn Anh⁴, Nguyễn Quốc Tuấn^{1,*}

¹*Department of Networks and Communications Systems, VNU University of Engineering and Technology*

²*Institute of Materials Science, VAST, 18 Hoàng Quốc Việt, Cầu Giấy, Hanoi, Vietnam*

³*Faculty of Telecommunications, Posts and Telecom. Inst. Tech., Hanoi city, Vietnam*

⁴*Computer Communications Lab. The University of Aizu, Aizu-Wakamatsu city, Fukushima, Japan*

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Abstract: In this paper, we investigate effects of Erbium-doped fiber amplifier (EDFA) amplified spontaneous emission (ASE) noise on the performance of multi-wavelength OCDMA-based Long-Reach Passive Optical Networks. In addition, other noise and interference such as shot noise, thermal noise, beat noise, and multiple-access interference (MAI) are included in our theoretical analysis and simulation. We found that the location of EDFA on the link between OLT and ONUs plays an important role in network design since it affects network performance. Analytical results show that, to achieve low bit error rate, the EDFA should be located around 10 to 20 km from OLT when total link distance of 90 km.

Keywords: Erbium-doped fiber amplifier (EDFA), optical code-division multiplexing (OCDM), amplified spontaneous emission (ASE), multiple-access interference (MAI).

1. Introduction

The explosive demand for bandwidth is leading to the deployment of passive optical networks (PONs), which are able to bring the high-capacity optical fiber closer to the residential homes and small businesses. Long-reach (LR) PON is a recently proposed cost-effective architecture for combining the metro

and access networks. This architecture allows the extension of access networks from today's standard of 20 km to 100 km with protection mechanism [1-3].

A number of LR optical access technologies have been proposed. Initially, the networks were single channel, where a single wavelength is shared between all users, using time division multiplexing (TDM). These networks were followed by wavelength division multiplexing (WDM) ones that shared a number of

* Corresponding author. Tel: 84-913301974.
E-mail: tuannq@vnu.edu.vn

wavelengths between groups of users. Recently, optical code-division multiplexing (OCDM) has been regarded as a promising candidate thanks to its advantages over conventional techniques, including asynchronous access efficient use of resource, scalability and inherent security [4, 5].

In OCDM, the signal can be encoded using the time domain, the frequency domain, or a combination of the two [6]. In a time-domain encoding system, the signal is encoded by time spreading of an optical pulse. The system is spectrally inefficient as a long code word is usually required to maintain a low cross-correlation. In the frequency domain, by using multiple wavelengths for signal encoding, spectral amplitude coding (SAC) OCDM [7, 8] can offer a better spectral efficiency. Another important advantage of SAC/OCDM is that multiple-access interference (MAI), in theory, can be eliminated by using a balance detection receiver. In addition, unlike other frequency-domain systems that use phase for signal encoding, SAC/OCDM can use incoherent sources, which allows for simpler and cheaper systems. This feature is very important, especially in the access network environment where construction cost is one of the most critical issues.

In this paper, we therefore propose a novel architecture of a LR-PON using SAC/OCDM. To reach a long transmission distance, an Erbium-doped fiber amplifier (EDFA) is located on the link between optical line terminal (OLT) and optical network units (ONUs). However such an EDFA also generates amplified spontaneous emission (ASE) noise, which will limit system performance to an electrical signal to noise ratio at the photodiode determined by the spontaneous-spontaneous and carrier-spontaneous beat noise. Thus, based on proposed architecture, we analyze the effects

of EDFA noise, i.e. ASE noise, on the performance of OCDM-based LR-PON. Other noise and interference such as shot noise, thermal noise, beat noise, and multiple-access interference (MAI) are also included in our theoretical analysis and simulation. In order to achieve a good performance, we will try to find the best location to put the EDFA in the network.

The rest of this paper is organized as follows. In Section II, we present the architecture of an OCDM-based LR-PON. The theoretical analysis of the performance of LR-PON is presented in Section III. In Section IV, we show the simulation setup of an OCDM-based LR-PON, the simulation results, and discussion. Finally, Section V concludes the paper.

2. OCDM-based LR-PON Architecture

A SAC/OCDM-based LR-PON architecture is illustrated in Fig. 1. It consists of a shared fiber that originates from an OLT. At a point close to the customer premises, a passive optical splitter is used to connect each ONU to the main fiber.

At the OLT, downstream traffics sending to K users are encoded by spectral encoders, which can be implemented using the well-studied fiber Bragg grating (FBG) structure [9]. The spectral encoders are controlled by different codes denoted as C_m with $m=1, 2, \dots, K$. At each spectral encoder, a broadband (multi-wavelength) source, whose number of wavelengths are N_w , is first on-off keying (OOK) modulated by binary data. Next, depending on the signature code (C_m), wavelengths corresponding to chips "1" in a signature code are blocked while others can

pass through. As a result, each binary bit "1" is represented by a multi-wavelength pulse while no signal is transmitted in case of binary bit "0". Multi-wavelength pulse from each encoder is then combined at a K: 1 combiner and then transmitted into the optical fiber. To compensate fiber loss and the various coupler losses, an EDFA optical amplifier is placed on the link at the distance of L_1 (km) from OLT while the distance from the EDFA amplifier to the splitter is L_2 (km). All wavelengths are amplified simultaneously while passing through the amplifier thanks to its large bandwidth. The average gain of optical amplifier is denoted as G .

Each ONU receives the signals not only from desired encoder (i.e., data signal) but also from remaining encoders (i.e., MAI signal). There are two decoders at each ONU. The first decoder has the same characteristic with the desired encoder while the second one has reverse characteristic. It means that all wavelengths corresponding to chips "0" of C_m are blocked by the second decoder.

The signature codes used in SAC/OCDM systems are designed to have a fixed in-phase cross-correlation value so that the number of wavelengths passing through each decoder, in the case of an interfering signal (from undesired decoders), are the same. Because the decoded signal from the two decoders is detected by two photodetectors (PD1 and PD2) connected in a balanced fashion on the additive and subtractive branches, all interfering signals (i.e., MAI) can be eliminated [7].

3. Theoretical Analysis

In this system, we use the Hadamard code, whose weight and in-phase cross correlation

can be represented by its length (N). Let C_m and C_n be two code vectors, the correlation between these two vectors can be expressed as.

$$R_{C_m, C_n} = \sum_{i=1}^N (C_{m,i} C_{n,i}) = \begin{cases} N/2 & (m = n) \\ N/4 & (m \neq n) \end{cases} \quad (1)$$

Let R refers to the responsivity of the photodiode and P_{tx} to transmitted optical power, N_w to number of wavelengths, K is number of active users, the data current generated by the optical data signal at the output of PD₁ and PD₂ can be respectively expressed as

$$I_{data}^+ = \frac{1}{2K} RG \frac{P_{tx}}{N_w} (N_w - \frac{N}{2}) 10^{-\alpha(L_1+L_2)/10} \quad (2)$$

$$I_{data}^- = \frac{1}{2K} RG \frac{P_{tx}}{N_w} (N_w - N) 10^{-\alpha(L_1+L_2)/10}$$

where α is the fiber attenuation coefficient in dB/km. The total data current, therefore, can be expressed as

$$I_{data} = I_{data}^+ - I_{data}^- = \begin{cases} \frac{1}{2K} RG \frac{P_{tx}}{N_w} \frac{N}{2} 10^{-\alpha(L_1+L_2)/10} & (\text{bit } 1) \\ 0 & (\text{bit } 0) \end{cases} \quad (3)$$

The photocurrents caused by the MAI signals from interfering encoders when they pass the PD1 and PD2 are given by

$$I_{MAI}^+ = I_{MAI}^- = \frac{1}{2K} RG \frac{P_{tx}}{N_w} (N_w - \frac{3N}{4}) 10^{-\alpha(L_1+L_2)/10} \quad (4)$$

Due to ASE that is caused by the amplifier, there is also ASE noise current at the output of two photodetectors, which can be expressed as

$$I_{ASE}^+ = I_{ASE}^- = \frac{1}{2K} R \eta f n_{sp} (G-1) B_{opt} 10^{-\alpha L_2/10} \quad (5)$$

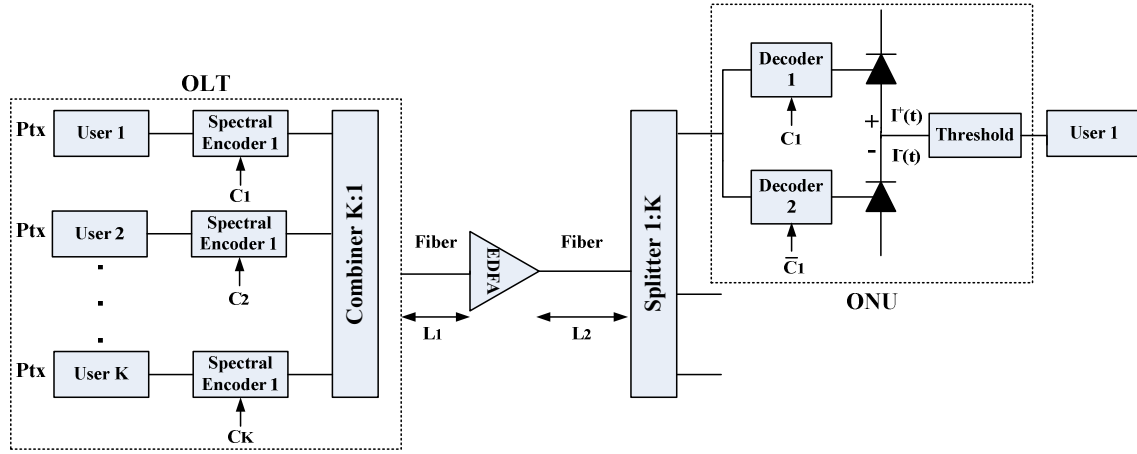


Fig. 1. Block diagram of a SAC/OCDM-based LR-PON.

Where h is Planck's constant; f is the optical frequency; B_{opt} is the optical bandwidth; and n_{sp} is the spontaneous-emission factor (or the population-inversion factor).

Other noise that should be taken into account at the ONU includes the thermal noise, shot noise, and beat noise [10]. First, the variance of the thermal noise can be written as

$$\sigma_{th}^2 = \frac{4K_B T B}{R_L} \quad (6)$$

Where, K_B is Boltzman's constant, T is the receiver temperature, B is the bit rate, and R_L is the load resistance.

Next, the variance of the shot noise, which is generated by data, ASE, and MAI signal, is given by

$$\begin{aligned} \sigma_{shot}^2 &= 2qB(I_{data}^+ + I_{data}^-) + 2qB(I_{MAI}^+ + I_{MAI}^-) \\ &\quad + 2qB(I_{ASE}^+ + I_{ASE}^-) \\ &= \frac{1}{K} qBRG \frac{P_{tx}}{N_w} (2N_w - \frac{3N}{2}) 10^{-\alpha(L_1+L_2)/10} \\ &\quad + \frac{2}{K} (K-1) qBRG \frac{P_{tx}}{N_w} (N_w - \frac{3N}{4}) 10^{-\alpha(L_1+L_2)/10} \\ &\quad + \frac{2}{K} qBRhfn_{sp}(G-1)B_{opt} 10^{-\alpha L_2/10} \end{aligned} \quad (7)$$

The last one is beat noise current. It consists of the signal-ASE beat noise, the ASE-ASE beat noise (beating between the spectral components of the added amplifier ASE), the MAI-ASE beat noise and the signal-signal beat noise. The variance of the beat noise is given by Eq. (8).

$$\begin{aligned}
\sigma_{beat}^2 &= (I_{data}^+ I_{ASE}^+ + I_{data}^- I_{ASE}^-) \frac{B}{B_{opt}} + \frac{1}{2} [(I_{ASE}^+)^2 + (I_{ASE}^-)^2] \frac{B(2B_{opt} - B)}{B_{opt}^2} \\
&+ (I_{MAI}^+ I_{ASE}^+ + I_{MAI}^- I_{ASE}^-) \frac{B}{B_{opt}} + \frac{1}{2} (K-1) (I_{data}^+ I_{MAI}^+ + I_{data}^- I_{MAI}^-) \frac{B(2B_{opt} - B)}{B_{opt}^2} \\
&+ \frac{1}{2} (K-1) \left(\frac{K}{2} - 1\right) [(I_{MAI}^+)^2 + (I_{MAI}^-)^2] \frac{B(2B_{opt} - B)}{B_{opt}^2} \\
&= \frac{1}{2K} R G \frac{P_{tx}}{N_w} \left(2N_w - \frac{3N}{2}\right) 10^{-\alpha(L_1+L_2)/10} I_{ASE} \frac{B}{B_{opt}} + \frac{B(2B_{opt} - B)}{B_{opt}^2} (I_{ASE})^2 \\
&+ \frac{1}{K} (K-1) R G \frac{P_{tx}}{N_w} \left(N_w - \frac{3N}{4}\right) 10^{-\alpha(L_1+L_2)/10} I_{ASE} \frac{B}{B_{opt}} \\
&+ \frac{1}{8K^2} (K-1) R^2 G^2 \left(\frac{P_{tx}}{N_w}\right)^2 \left[N_w - \frac{N}{2}\right] \left[N_w - \frac{3N}{4}\right] \\
&+ (N_w - N) \left[N_w - \frac{3N}{4}\right] \frac{B(2B_{opt} - B)}{B_{opt}^2} 10^{-\alpha(L_1+L_2)/10} \\
&+ \frac{1}{4K^2} (K-1) \left(\frac{K}{2} - 1\right) R^2 G^2 \left(\frac{P_{tx}}{N_w}\right)^2 \left(N_w - \frac{3N}{4}\right) \frac{B(2B_{opt} - B)}{B_{opt}^2} 10^{-\alpha(L_1+L_2)/10} \quad (8)
\end{aligned}$$

The total variance of the noise current is the sum of all variances of thermal noise, shot noise, beat noise and can be written as

$$\sigma_{total}^2 = \sigma_{th}^2 + \sigma_{shot}^2 + \sigma_{beat}^2 \quad (7)$$

Finally, the bit error rate (BER) can be calculated as

$$BER = \frac{1}{2} \operatorname{erfc}\left(\frac{Q}{\sqrt{2}}\right) \quad (8)$$

Where $\operatorname{erfc}(\cdot)$ is the complementary error function, and Q is written as [11]

$$Q = \frac{I_{data}(1) - I_{data}(0)}{\sqrt{\sigma_{total}^2(1) + \sigma_{total}^2(0)}} \quad (9)$$

where $I_{data}(1)$ and $I_{data}(0)$ are the data currents that can be derived from Eq. (3) for bit "1" and bit "0", respectively. Both $\sigma_{total}^2(1)$ and $\sigma_{total}^2(0)$ are calculated using Eq. (9). However, when $\sigma_{total}^2(0)$ is computed, the value of I_{data}^+ and I_{data}^- should be zero in all related equations.

Figure 2 shows noise power as a function of the transmitted power for bit rate of 1 Gbps, 3 users, optical bandwidth of 100 nm and optical amplifier gain of 20 dB. The noise terms contributing significantly to σ_{total}^2 are drawn separately. The beating of the signal-signal and the signal-ASE clearly dominate all other noise terms. It can be said that ASE noise has significantly impact on performance of the system.

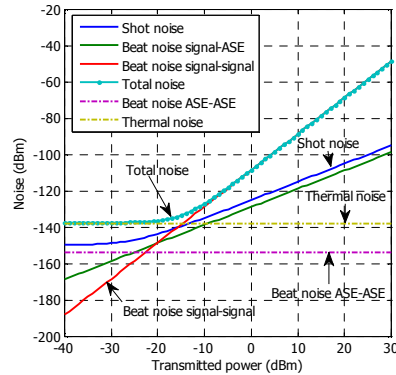


Fig. 2. Noise power as a function of the transmitted power with K=3 users, Rb=1 Gbps, G=20 dB.

4. Simulation setup and results

4.1. Simulation Setup

The simulation of SAC/OCDM-based LR-PON is carried out on OptiSystem, a comprehensive software design suite that enables users to plan, test, and simulate optical links in the transmission layer of modern optical networks [12]. The block diagram of the simulation model is shown in Fig. 3. The signal spectrums at the outputs of the modulator, encoder and decoders are also illustrated in the figure.

Three downstream traffics are generated by three PRBS generators, which generate pseudo random bit sequences. These bit sequences are then used to control NRZ generators to generate non-return-to-zero signals. OOK modulation between a NRZ signal and a multi-wavelength signal that is generated by a white light source is carried out by using a Mach-Zehnder modulator. Finally, multi-wavelength OOK signals are encoded at encoders, which are constructed from FBGs.

A power combiner will combine the signals from different encoders then transmit them into the first optical fiber. The signals then will be amplified by an EDFA amplifier and input into the second optical fiber.

In the receiver side, two power splitters are used. The first one is responsible to deliver the signals to all ONUs. The second one is located at each ONU to split the received signals into two parts for two decoders, which are also constructed from FBGs. Decoded signals are converted into photocurrents by using two PIN photodetector that are connected to a electrical subtractor to create a balance detector. Finally, BER of the received signal is analyzed by using a BER analyzer in combination with a low pass Bessel filter.

4.2. Simulation Results

Simulations have been carried out to study the effects of ASE noise and the position of EDFA amplifier on the performance of SAC/OCDM-based LR-PON. Key parameters used for this simulation are listed in Table 1.

Table 1: Parameters used for system simulations.

Name	Symbol	Value
Boltzmann's constant	K_B	1.38×10^{-23} W/K/Hz
Electron charge	q	1.6×10^{-19} C
Load resistor	R_L	1000 Ω
Receiver temperature	T	300 K
PD responsivity	\mathcal{R}	1 A/W
Length of code word	N	8
Number of wavelengths	N_w	17
Number of users	K	3
Bit rate per user	R_b	1 Gbps

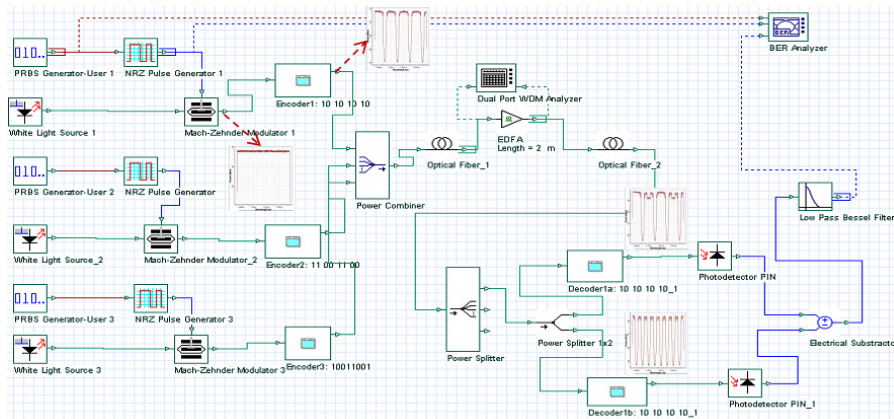


Figure 3. Simulation model of a SAC/OCDMA-based LR-PON.

We can observe spectrum of signals at the outputs of *modulator, encoder and decoders* as shown in Fig. 3. After going through the encoder, spectrum of signal is removed $N/2$ (i.e., 4) wavelengths. It will be unchanged while passing through decoder 1 and is further removed $N/2$ wavelengths while passing through decoder 2. Thus, the remaining wavelengths in spectrum of the signal at the output of decoder 2 are $(N - N_w)$.

In figure 4 and 5, we fix $G = 20$ dB and total link distance of 90 km. We investigate BER versus transmitted power for different two values of L_1 ($L_1 = 30$ km and $L_1 = 60$ km) from OLT to ONUs. We evaluate BER for two cases, with and without ASE noise. It is seen that the effect of ASE increases with distance L_1 . In these figures, dashed lines are the simulation results and solid lines are the theoretical results. They are rather close (separated by approximately 0.5 dB). That means the BER calculation of the simulation system is correct. More specially, the power penalty due to ASE noise at BER 10^{-9} is about 2 dB when $L_1 = 30$ km. When $L_1 = 60$ km, it increase to 4 dB. It is because, according to Eq. 5, ASE noise current is inversely proportional to L_2 . It means that I_{ASE} strong when L_2 is short or L_1 is large. It is the same for both simulation and theoretical results.

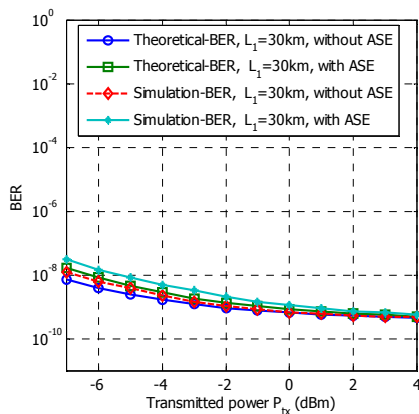


Fig. 4. BER vs. transmitted power (P_{tx}) with $K=3$ users, $R_b=1$ Gbps, $L_1=30$ km.

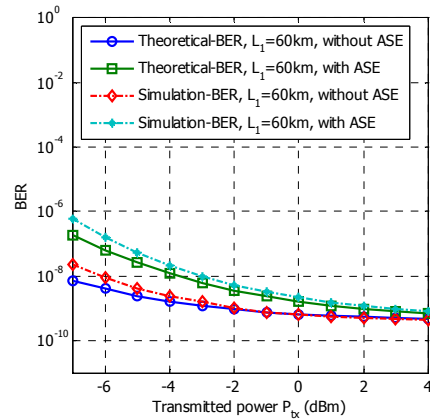


Fig. 5. BER vs. transmitted power (P_{tx}) with $K=3$ users, $R_b=1$ Gbps, $L_1=60$ km.

Figure 6 and 7 show the dependence of BER on the position of EDFA amplifier on link for two different values of transmitted power, $P_{tx} = -4$ dBm and $P_{tx} = -2$ dBm. We can see that, in the absence of ASE, BER reduces when L_1 increases. However, when ASE noise is considered, the longer L_1 is, the worse BER is. The values of L_1 at which the lowest BER can be achieved is the range of 10 km to 20 km. Here, dashed simulation BER lines and solid theoretical lines are parallel and rather close, that means simulation results are correct.

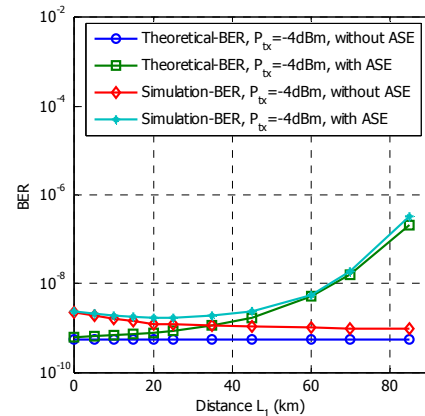


Fig. 6. BER vs. the link distance (L_1) with $K=3$ users, $R_b=1$ Gbps, $G=20$ dB, $P_{tx}=-4$ dBm, and total link distance $L_1+L_2=90$ km.

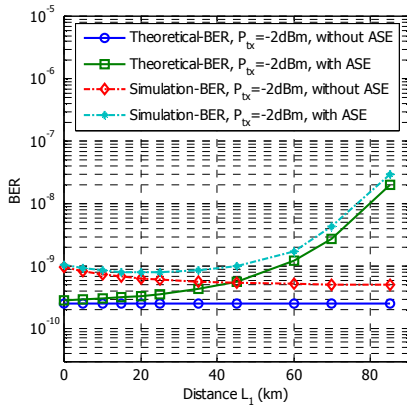


Fig. 7. BER vs. the link distance (L_1) with $K=3$ users, $R_b=1$ Gbps, $G=20$ dB, $P_{tx}=-2$ dBm, and total link distance $L_1+L_2=90$ km.

Figure 8 shows the BER of the system versus the number of active users when each user bit rate is 1 Gbps and transmitted power $P_{tx}=-4$ dBm for two different values of the link distance L_1 (30 and 60 km), with and without ASE noise. It is seen that when $L_1 = 30$ km then two curves are quite close to each other. However, the number of active users will decrease when link distance L_1 increase to 60 km in the present of ASE noise. That means, the effect of the position of EDFA and ASE noise on number of active users are considerable.

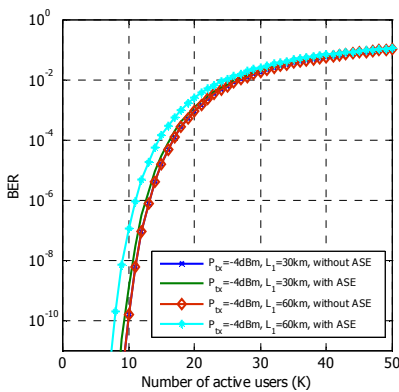


Fig. 8. BER vs. the number of active users (K) with $R_b=1$ Gbps, $G=20$ dB, $P_{tx}=-4$ dBm, and total link distance $L_1+L_2=90$ km.

Other useful information for network design can be obtained from Fig. 9, where the required EDFA gain that is corresponding to a specific distance of L_1 at $BER=10^{-9}$ can be found. Based on this result, we are able to determine the required EDFA gain corresponding to the specific value of L_1 or the location of EDFA on the link.

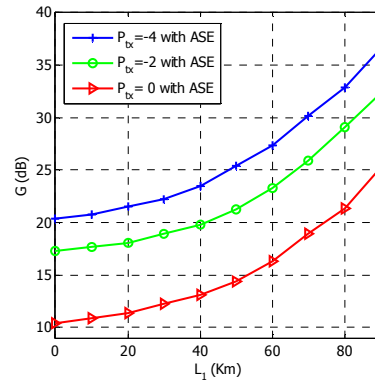


Fig. 9. G vs. the link distance (L_1) with $K=3$ users, $R_b=1$ Gbps, $BER=10^{-9}$, and total link distance $L_1+L_2=90$ km.

5. Conclusion

In this paper, we have proposed a model of LR-PON using multi-wavelength OCDM and EDFA. Moreover, we analyzed the effects of ASE noise on the performance of OCDM-based LR-PON. Other noise and interference such as shot noise, thermal noise, beat noise, and MAI are included in our theoretical analysis and simulation. We found that the location of EDFA on the link between OLT and ONUs plays an important role in network design since it affects on the network performance. According to the numerical results, to achieve low bit error rate, the EDFA should be located around 10 to 20 km from OLT when total link distance (i.e., $L_1 + L_2$) of 90 km.

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Ảnh hưởng của nhiễu phát xạ tự phát được khuếch đại và vị trí của bộ khuếch đại sợi pha tạp Erbium đến hiệu năng của mạng quang thụ động khoảng cách dài dựa trên kỹ thuật ghép kênh phân chia theo mã quang đa bước sóng

Bùi Trung Ninh¹, Phạm Văn Hội², Đặng Thế Ngọc³,
Phạm Tuấn Anh⁴, Nguyễn Quốc Tuấn¹

¹Bộ môn Hệ thống viễn thông, Trường Đại học Công nghệ, ĐHQGHN, 144 Xuân Thủy, Hà Nội, Việt Nam

²Viện Khoa học Vật liệu, Viện Hàn lâm Khoa học và Công nghệ Việt Nam, 18 Hoàng Quốc Việt, HN, VN

³Khoa Viễn thông 1, Học viện Công nghệ Bưu chính Viễn thông, Hà Nội

⁴Phòng thí nghiệm Truyền thông máy tính, Đại học Aizu, Nhật Bản

Tóm tắt: Trong bài báo này, chúng tôi khảo sát các ảnh hưởng của nhiễu phát xạ tự phát do bộ khuếch đại EDFA gây ra đến hiệu năng của mạng quang thụ động khoảng cách dài dựa trên đa truy

nhập phân chia theo mã quang đa bước sóng. Ngoài ra, các nhiễu khác như nhiễu hạt, nhiễu nhiệt, nhiễu giữa các tín hiệu tần số khác nhau, và nhiễu đa truy cập sẽ được thảo luận trong phần tính toán lý thuyết và mô phỏng. Chúng tôi nhận thấy rằng vị trí của bộ khuếch đại EDFA trên tuyến giữa đầu cuối đường dây quang (OLT) và thiết bị mạng quang (ONU) đóng vai trò quan trọng trong việc thiết kế mạng bởi vì nó ảnh hưởng đến hiệu năng của mạng. Các kết quả phân tích cho biết, để đạt được tỉ lệ lỗi bit thấp, bộ khuếch đại nên đặt trong khoảng từ 10 đến 20 km từ OLT khi tổng khoảng cách tuyến là 90 km.

Từ khóa: Bộ khuếch đại sợi pha tạp Erbium (EDFA), ghép kênh phân chia theo mã quang (OCDM), phát xạ tự phát được khuếch đại (ASE), nhiễu đa truy cập (MAI).